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Modified projective synchronization with complex scaling factors of uncertain real chaos and complex chaos*

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To increase the variety and security of communication, we present the definitions of modified projective synchronization with complex scaling factors (CMPS) of real chaotic systems and complex chaotic systems, where complex scaling factors establish a link between real chaos and complex chaos. Considering all situations of unknown parameters and pseudo-gradient condition, we design adaptive CMPS schemes based on the speed-gradient method for the real drive chaotic system and complex response chaotic system and for the complex drive chaotic system and the real response chaotic system, respectively. The convergence factors and dynamical control strength are added to regulate the convergence speed and increase robustness. Numerical simulations verify the feasibility and effectiveness of the presented schemes.

Keywords: modified projective synchronization, complex scaling factors, complex chaotic systems, speedgradient method

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1. Introduction

Since the seminal work by Pecora and Carrol,^[1] chaos synchronization has been widely investigated for applications in secure communication.^[2-5] Since Fowler et al.^[6] introduced the complex Lorenz equations, the complex Chen and Lü systems have been proposed. These chaotic systems which involve complex variables are used to describe the physics of a detuned laser, rotating fluids, disk dynamos, electronic circuits, and particle beam dynamics in high energy accelerators. Now complex systems have played an important role in many branches of physics, e.g. fluids, superconductors, plasma physics, geophysical fluids, modulated optical waves, and electromagnetic fields.^[7] The adoption of a complex chaotic system has also been proposed for secure communication, and the complex variables (doubling the number of variables) increase the contents and security of the transmitted information.^[8] The idea is similar to the real chaotic system, i.e., chaotic signal is used as a carrier and transmitted together with an information signal to a receiver, and at the receiver end chaos synchronization is employed to recover the information signal.^[9] Hence, the synchronization of complex chaotic systems has attracted greater attention in the last few decades, such as phase synchronization and antiphase synchronization,^[10] complete synchronization (CS),^[11] anti-synchronization (AS),^[12,13] lag synchronization (LS),^[14] modified function projective synchronization(MFPS),^[15] etc.

Recently, Hu *et al.*^[16] observed hybrid projective synchronization (HPS), in which the different state variables can synchronize up to different scaling factors, in coupled partially

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linear chaotic complex nonlinear systems without adding any control term. Mahmoud and Mahmoud^[17] investigated the phenomenon of projective synchronization (PS) and modified projective synchronization (MPS) of hyperchaotic attractors of hyperchaotic complex Lorenz system by active control. PS is a situation in which the state variables of the drive and response systems synchronize up to a real constant scaling factor δ (δ is a constant). MPS is defined if the responses of the synchronized dynamical states synchronize up to a real constant scaling matrix. Later, Liu Ping and Liu Shu-Tang^[18] presented full state hybrid projective synchronization (FSHPS) with real scaling factors for two complex chaotic systems according to the definition of FSHPS for real chaotic systems.^[19,20] In fact, the FSHPS is MPS of all state variables.

However, the above studies only touch on real scaling factors. In fact, the scaling factors can be complex for complex dynamical systems. The complex scaling factors establish a link between real chaotic systems and complex chaotic systems. If the drive system is real, we can adopt a complex system to synchronize the real drive system with complex scaling factors. It means that we obtain a complex signal from real chaotic signal multiplied by complex scaling factors, then the real part and the imaginary part of this complex signal are transmitted together with an information signal to a receiver, and at the receiver, we employ a complex system to synchronize to recover the information signal. Therefore, it is easy to transmit a complex signal. If the drive system is complex, we can adopt a real system to synchronize the real (imaginary) part of the product of complex drive system and complex scal-

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ing factors. It means the real (imaginary) part of this product is transmitted together with an information signal to a receiver, and at the receiver, we employ a real response system to synchronize this real (imaginary) part to recover the information signal. It will increase the range of choosing chaotic generators in the transmitters and receivers, thus an interceptor is harder to crack information sources.

In application to secure communications. Chee and Xu^[21] extended binary digital to M-nary digital communication for achieving fast communication by manipulating the scaling feature of projective synchronization. The unpredictability of the scaling factor in projective synchronization can additionally enhance the security of communication. Since the complex scaling factors are arbitrary and more unpredictable than real scaling factors and the operations of complex numbers are complicated, the possibility that an interceptor extracts the information from the transmitted signal is greatly less than real scaling factors. Moreover, modified projective synchronization with complex scaling factors (CMPS) of real chaotic systems and complex chaotic systems will increase the complexity and scope of the synchronization, which will also increase security and variety of communications. Therefore, it is significant to study CMPS of real chaotic systems and complex chaotic systems. However, to the best of our knowledge, the CMPS has rarely been explored.

In practice, some systems' parameters cannot be exactly known, and the synchronization will be destroyed. For example, the receiver in secure communication is definitely suffering from all kinds of uncertainties such as uncertain parameters, which no doubt affects the precision of the communication. Therefore, we consider chaotic systems with unknown parameters. The adaptive control is one popular and useful approach to control and synchronize nonlinear chaotic systems with unknown parameters. Many researches^[22-25] about the adaptive control of real uncertain chaotic systems are based on speed-gradient (SG) methodology. As for complex chaotic systems, Liu Shu-Tang and Liu Ping^[12] preliminarily applied the SG method to the anti-synchronization of a class of uncertain chaotic complex systems; they also studied the FSHPS scheme with real scaling factors for a class of uncertain chaotic complex systems based on the SG method.^[18] However, the adaption laws in these investigations do not contain convergence factors and pseudo-gradient conditions. Especially, they adopted the fixed control strength in error feedback wherever the initial points start, thus the strength must be maximal, which means a kind of waste in practice.^[26] In a word, they did not indicate simple SG method clearly, and they did not consider convergence factors, pseudo-gradient condition, and the adaptive control strength. Besides, the number of unknown parameters in drive and response systems was the same, and either both were real or both were complex.

Inspired by the above discussion, we present CMPS of uncertain real chaotic systems and complex chaotic systems, considering all situations of unknown parameters based on the SG method with convergence factors, pseudo-gradient condition, and dynamical control strength.

The rest of the paper is organized as follows: the SG method is introduced in Section 2. We give the definition of CMPS of real drive chaotic system and complex response chaotic system and design the corresponding adaptive CMPS schemes in Section 3. In Section 4, we discuss the definition of CMPS of complex drive chaotic system and the real response chaotic system and corresponding CMPS schemes. In simulations, we realize CMPS of uncertain real hyperchaotic Rössler system and complex hyperchaotic Lorenz system and of complex Lorenz drive system and real Lorenz response system, respectively. Finally, some conclusions are given in Section 6.

2. Speed-gradient method

Consider the following *n*-dimensional real chaotic system

$$\dot{\boldsymbol{x}} = \boldsymbol{\phi}(\boldsymbol{x}, \boldsymbol{\theta}, t), \tag{1}$$

where $\boldsymbol{x} = (x_1, x_2, ..., x_n)^T$ is a real state vector (T denotes transpose), $\boldsymbol{\theta}$ is a real matrix of unknown parameters. To output the desired signal $\boldsymbol{x}^*(t)$, we consider the error criterion function $\boldsymbol{\Phi}(t) = \boldsymbol{\Phi}(\boldsymbol{x}, t)$ (If $\boldsymbol{x}(t) \rightarrow \boldsymbol{x}^*(t), \boldsymbol{\Phi}(\boldsymbol{x}, t) \rightarrow 0$) which is a scalar smooth nonnegative function. Its time derivative is

$$\omega(\theta,t) = \frac{\partial \Phi(\boldsymbol{x},t)}{\partial t} + \nabla_{\boldsymbol{x}} \Phi(\boldsymbol{x},t) \phi(\boldsymbol{x},\theta,t).$$
(2)

According to the speed-gradient method, the change of θ is along the opposite gradient direction of $\omega(\theta, t)$ in θ . The most general, i.e., the so-called combined form of the SG algorithm looks as follows:

$$\frac{\mathrm{d}}{\mathrm{d}t}(\boldsymbol{\theta} + \boldsymbol{\varphi}(t)) = -\Gamma \nabla_{\boldsymbol{\theta}} \boldsymbol{\omega}(\boldsymbol{\theta}, t), \tag{3}$$

where Γ is a corresponding positive-definite gain matrix, and $\varphi(t)$ is a certain vector function satisfying the pseudogradient condition

$$\varphi^{\mathrm{T}}(t)\nabla_{\theta}\omega(\theta,t) \ge 0.$$
 (4)

Equation (3) can also be written in the finite-integral form as

$$\boldsymbol{\theta} = -\boldsymbol{\varphi}(t) - \boldsymbol{\Gamma} \int_0^t \nabla_{\boldsymbol{\theta}} \boldsymbol{\omega}(\boldsymbol{\theta}, \boldsymbol{\alpha}) \, \mathrm{d}\boldsymbol{\alpha}.$$
 (5)

The general stability theorem for combined SG law (3) is formulated below:

Lemma 1^[22] Consider the systems (1) and (3) under the following assumptions:

Al) $\phi(x, \theta, t)$ and $\nabla_{\theta} \omega(\theta, t)$ are bounded together with their partial derivatives on any bounded set of states (x, θ) of the systems (1) and (3) uniformly in $t \ge 0$ (regularity condition);

A2) $\omega(\theta, t)$ is convex in θ (convexity condition);

A3) There exist a real constant matrix θ^* and scalar uniformly continuous in each bounded region function $\rho(x) \ge 0$, $\rho(0) = 0$ such that inequality $\omega(\theta^*, t) \le -\rho(x)$ holds for all $x \in \mathbb{R}^n$ (achievability condition);

A4) If $\Phi(x,t)$ is bounded then x(t) is bounded as well (boundedness condition);

Then each trajectory $(\boldsymbol{x}(t), \boldsymbol{\theta}(t))$ of systems (1), (3), and (5) is bounded and $\lim_{t \to \infty} \rho(\boldsymbol{x}(t)) = 0$.

The proof is presented in the appendix of the literature^[22] and thus is omitted.

3. CMPS schemes of real drive systems and complex response systems

3.1. Mathematical model and problem descriptions

Consider the following *n*-dimensional real drive chaotic system with unknown parameters,

$$\dot{\boldsymbol{z}} = \boldsymbol{G}(\boldsymbol{z})\boldsymbol{B} + \boldsymbol{g}(\boldsymbol{z}), \tag{6}$$

where $\boldsymbol{z} = (z_1, z_2, ..., z_n)^{\mathrm{T}}$ is a real state vector, $\boldsymbol{B} = (b_1, b_2, ..., b_s)^{\mathrm{T}}$ is an $s \times 1$ real vector of unknown parameters, and $\boldsymbol{G}(\boldsymbol{z})$ is an $n \times s$ real matrix, and $\boldsymbol{g} = (g_1, g_2, ..., g_n)^{\mathrm{T}}$ is a vector of real nonlinear function.

The complex response chaotic system is depicted as,

$$\dot{\boldsymbol{w}} = \boldsymbol{F}(\boldsymbol{w})\boldsymbol{A} + \boldsymbol{f}(\boldsymbol{w}) + \boldsymbol{v}, \qquad (7)$$

where $\boldsymbol{w} = (w_1, w_2, \dots, w_n)^T$ is a complex state vector, and $\boldsymbol{w} = \boldsymbol{w}^r + j\boldsymbol{w}^i$. Superscripts r and i stand for the real and imaginary parts of \boldsymbol{w} , respectively. Set $w_1 = u_1 + ju_2$, $w_2 = u_3 + ju_4, \dots, w_n = u_{2n-1} + ju_{2n}$, and $\boldsymbol{w}^r = (u_1, u_3, \dots, u_{2n-1})^T$, $\boldsymbol{w}^i = (u_2, u_4, \dots, u_{2n})^T$. $\boldsymbol{f} = (f_1, f_2, \dots, f_n)^T$ is a vector of complex nonlinear function, $\boldsymbol{F}(\boldsymbol{w})$ is an $n \times m$ complex matrix and its elements are functions of complex state variables, and $\boldsymbol{A} = (a_1, a_2, \dots, a_m)^T$ is an $m \times 1$ real (or complex) vector of unknown parameters. The designed controller is $\boldsymbol{v} = \boldsymbol{v}^r + j\boldsymbol{v}^i$, where $\boldsymbol{v}^r = (v_1, v_3, \dots, v_{2n-1})^T$, $\boldsymbol{v}^i = (v_2, v_4, \dots, v_{2n})^T$.

According to the definition of MPS^[17] and FSHPS^[18] with real scaling factors of two chaotic complex systems, we give the definition of CMPS of real drive chaotic systems and complex response chaotic systems.

Definition 1 For the drive system (6) and response system (7), if there exists a complex constant matrix $H = \text{diag}\{h_1 + jh_2, h_3 + jh_4, \dots, h_{2n-1} + jh_{2n}\}$ such that

$$\begin{split} &\lim_{t \to \infty} \|\boldsymbol{e}(t)\|^2 \\ &= \lim_{t \to \infty} \|\boldsymbol{w}(t) - \boldsymbol{H}\boldsymbol{z}(t)\|^2 \\ &= \lim_{t \to \infty} (\|\boldsymbol{w}(t)^{\mathrm{r}} - \boldsymbol{H}^{\mathrm{r}}\boldsymbol{z}(t)\|^2 + \|\boldsymbol{w}(t)^{\mathrm{i}} - \boldsymbol{H}^{\mathrm{i}}\boldsymbol{z}(t)\|^2) \\ &= 0, \end{split}$$

where e(t) is the error vector, $e^{r}(t) = (e_1, e_3, \dots, e_{2n-1})^{T}$, $e^{i}(t) = (e_2, e_4, \dots, e_{2n})^{T}$, $H^{r} = \text{diag}\{h_1, h_3, \dots, h_{2n-1}\}$, $H^{i} = \text{diag}\{h_2, h_4, \dots, h_{2n}\}$, and $\|\cdot\|$ denotes the Euclidean norm of a vector, then the real drive system (6) and complex response system (7) are CMPS, and $h_1 + jh_2, h_3 + jh_4, \dots, h_{2n-1} + jh_{2n}$ are complex scaling factors. If there exists $w_l \in R$ $(l = 1, 2, \dots, n)$, we select $h_{2l} = 0$ to avoid increasing a new imaginary part in the response system.

The control objective is to design an adaptive controller v such that the response complex system (7) can synchronize the drive real system (6) asymptotically in sense of the CMPS.

3.2. Adaptive CMPS schemes

If *A* is a real vector, according to the SG method, we have the following theorem.

Theorem 1 If the adaptive controller is designed as

$$v = -F(w)\hat{A} - f(w) + HG(z)\hat{B} + Hg(z) + Ke$$

= $-F(w)^{r}\hat{A} - f(w)^{r} + H^{r}G(z)\hat{B} + H^{r}g(z) + Ke^{r}$
+ $[-F(w)^{i}\hat{A} - f(w)^{i} + H^{i}G(z)\hat{B}$
+ $H^{i}g(z) + Ke^{i}],$ (9)

where $\mathbf{K} = \text{diag}(k_1, k_2, \dots, k_n)$ is the real control strength matrix and \hat{A} , \hat{B} are the estimated values of A and B, respectively; and the adaptive laws are selected as

$$\begin{cases} \hat{A} = -\varphi_{\hat{A}}(t) - \eta \int_{0}^{t} \nabla_{\hat{A}} \omega(\hat{A}, \hat{B}, \alpha) d\alpha, \\ \hat{B} = -\varphi_{\hat{B}}(t) - \tau \int_{0}^{t} \nabla_{\hat{B}} \omega(\hat{A}, \hat{B}, \alpha) d\alpha, \\ \dot{k}_{l} = -\gamma_{l} [e_{l}^{r}(t)^{2} + e_{l}^{i}(t)^{2}], \quad l = 1, 2, \dots, n, \end{cases}$$
(10)

where

$$\nabla_{\hat{A}}\omega(\hat{A},\hat{B},t) = -(F^{\mathrm{T}}(w)^{\mathrm{r}},F^{\mathrm{T}}(w)^{\mathrm{i}})\begin{bmatrix}e^{\mathrm{r}}\\e^{\mathrm{i}}\end{bmatrix},\qquad(11)$$
$$\nabla_{\hat{B}}\omega(\hat{A},\hat{B},t) = ((H^{\mathrm{r}}G(z))^{\mathrm{T}},(H^{\mathrm{i}}G(z))^{\mathrm{T}})\begin{bmatrix}e^{\mathrm{r}}\\e^{\mathrm{i}}\end{bmatrix},\qquad(12)$$

and $\varphi_{\hat{A}}(t) = \lambda \nabla_{\hat{A}} \omega(\hat{A}, \hat{B}, t), \quad \varphi_{\hat{B}}(t) = \zeta \nabla_{\hat{B}} \omega(\hat{A}, \hat{B}, t)$ which satisfy the pseudogradient condition, $\lambda = \text{diag}(\lambda_1, \lambda_2, ..., \lambda_n), \quad \eta = \text{diag}(\eta_1, \eta_2, ..., \eta_n), \quad \zeta = \text{diag}(\zeta_1, \zeta_2, ..., \zeta_n), \quad \tau = \text{diag}(\tau_1, \tau_2, ..., \tau_n), \text{ and } \gamma = \text{diag}(\gamma_1, \gamma_2, ..., \gamma_n)$ are the corresponding convergence factor matrixes and their elements are positive real constants, then the complex response system (7) will synchronize the real drive system (6) in sense of CMPS asymptotically, and \hat{A} , \hat{B} converge to constant vectors.

Proof From Eqs. (6), (7), and (9), we have

$$\dot{e} = \dot{w} - \dot{z}$$

$$= F(w)A + f(w) - F(w)\hat{A} - f(w)$$

$$+ HG(z)\hat{B} + Hg(z) + Ke - HG(z)B - Hg(z)$$

$$= F(w)(A - \hat{A}) - HG(z)(B - \hat{B}) + Ke$$

$$= F(w)\tilde{A} - HG(z)\tilde{B} + Ke, \qquad (13)$$

where $\tilde{A} = A - \hat{A} = (\tilde{a}_1, \tilde{a}_2, ..., \tilde{a}_m)^T$ and $\tilde{B} = B - \hat{B} = (\tilde{b}_1, \tilde{b}_2, ..., \tilde{b}_s)^T$ are the errors between the true values and estimated values of unknown parameters. Setting $\Psi(z) = HG(z)$, we get $\Psi(z)^r = H^rG(z)$, and $\Psi(z)^i = H^iG(z)$. Therefore, we have $\dot{e}^r = F(w)^r \tilde{A} - \Psi(z)^r \tilde{B} + Ke^r$, $\dot{e}^i = F(w)^i \tilde{A} - \Psi(z)^i \tilde{B} + Ke^i$.

We introduce the following nonnegative Lyapunov function as

$$V(\boldsymbol{e},t) = \frac{1}{2} [(\boldsymbol{e}^{\mathrm{r}})^{\mathrm{T}} \boldsymbol{e}^{\mathrm{r}} + (\boldsymbol{e}^{\mathrm{i}})^{\mathrm{T}} \boldsymbol{e}^{\mathrm{i}}] + \frac{1}{2} \boldsymbol{\eta}^{-1} (\boldsymbol{A} - \hat{\boldsymbol{A}} - \boldsymbol{\varphi}_{\hat{A}}(t))^{2} + \frac{1}{2} \boldsymbol{\tau}^{-1} (\boldsymbol{B} - \hat{\boldsymbol{B}} - \boldsymbol{\varphi}_{\hat{B}}(t))^{2} + \frac{1}{2} \sum_{l=1}^{n} \frac{1}{\boldsymbol{\eta}} (k_{l} + L)^{2}, \quad (14)$$

where L is an arbitrary large positive constant. From Eqs. (10)-(12), we have

$$\frac{\mathrm{d}}{\mathrm{d}t}(\tilde{A}-\varphi_{\hat{A}}(t))=-\frac{\mathrm{d}}{\mathrm{d}t}(\hat{A}+\varphi_{\hat{A}}(t))=\eta\nabla_{\hat{A}}\omega(\hat{A},\hat{B},t)$$

and

$$\frac{\mathrm{d}}{\mathrm{d}t}(\tilde{\boldsymbol{B}}-\boldsymbol{\varphi}_{\hat{\boldsymbol{B}}}(\boldsymbol{t}))=-\frac{\mathrm{d}}{\mathrm{d}t}(\hat{\boldsymbol{B}}+\boldsymbol{\varphi}_{\hat{\boldsymbol{B}}}(\boldsymbol{t}))=\tau\nabla_{\hat{\boldsymbol{B}}}\boldsymbol{\omega}(\hat{\boldsymbol{A}},\hat{\boldsymbol{B}},t),$$

then

$$\dot{V} = (\dot{\boldsymbol{e}}^{\mathrm{r}})^{\mathrm{T}}\boldsymbol{e}^{\mathrm{r}} + (\dot{\boldsymbol{e}}^{\mathrm{i}})^{\mathrm{T}}\boldsymbol{e}^{\mathrm{i}} - \tilde{\boldsymbol{A}}[(F^{\mathrm{T}})^{\mathrm{r}}\boldsymbol{e}^{\mathrm{r}} + (F^{\mathrm{T}})^{\mathrm{i}}\boldsymbol{e}^{\mathrm{i}}] - \lambda \nabla_{\hat{\boldsymbol{A}}} \omega(\hat{\boldsymbol{A}}, \hat{\boldsymbol{B}}, t)^{2} + \tilde{\boldsymbol{B}}[(\boldsymbol{\Psi}^{\mathrm{T}})^{\mathrm{r}}\boldsymbol{e}^{\mathrm{r}} + (\boldsymbol{\Psi}^{\mathrm{T}})^{\mathrm{i}}\boldsymbol{e}^{\mathrm{i}}] - \varsigma \nabla_{\hat{\boldsymbol{B}}} \omega(\hat{\boldsymbol{A}}, \hat{\boldsymbol{B}}, t)^{2} - \sum_{l=1}^{n} (k_{l} + L)[\boldsymbol{e}_{l}^{\mathrm{r}}(t)^{2} + \boldsymbol{e}_{l}^{\mathrm{i}}(t)^{2}] < (\boldsymbol{F}^{\mathrm{r}} \tilde{\boldsymbol{A}} - \boldsymbol{\Psi}^{\mathrm{r}} \tilde{\boldsymbol{B}} + \boldsymbol{K} \boldsymbol{e}^{\mathrm{r}})^{\mathrm{T}} \boldsymbol{e}^{\mathrm{r}} + (\boldsymbol{F}^{\mathrm{i}} \tilde{\boldsymbol{A}} - \boldsymbol{\Psi}^{\mathrm{i}} \tilde{\boldsymbol{B}} + \boldsymbol{K} \boldsymbol{e}^{\mathrm{i}})^{\mathrm{T}} \boldsymbol{e}^{\mathrm{i}} - \tilde{\boldsymbol{A}}[(F^{\mathrm{T}})^{\mathrm{r}} \boldsymbol{e}^{\mathrm{r}} + (F^{\mathrm{T}})^{\mathrm{i}} \boldsymbol{e}^{\mathrm{i}}] + \tilde{\boldsymbol{B}}[(\boldsymbol{\Psi}^{\mathrm{T}})^{\mathrm{r}} \boldsymbol{e}^{\mathrm{r}} + (\boldsymbol{\Psi}^{\mathrm{T}})^{\mathrm{i}} \boldsymbol{e}^{\mathrm{i}}] - \sum_{l=1}^{n} k_{l} [\boldsymbol{e}_{l}^{\mathrm{r}}(t)^{2} + \boldsymbol{e}_{l}^{\mathrm{i}}(t)^{2}] - L \|\boldsymbol{e}\|^{2} = -L \|\boldsymbol{e}\|^{2}.$$
(15)

Conditions Al) and A2) are valid since the right-hand sides of Eqs. (9), (10), and (13) are smooth and linear in \hat{A} and \hat{B} . Condition A3) is valid since for the constant matrixes A and B we have $\dot{V} < -L||e||^2$, where $L||e||^2 \ge 0$. The validity of condition A4) follows from the radial unboundedness of the objective function (14) and boundedness of the trajectories of the drive model (6). Since all conditions of Lemma 1 are satisfied we conclude that w(t), \hat{A} , and \hat{B} are bounded, and $\lim_{t\to\infty} ||e(t)||^2 = 0$. We realize CMPS of system (6) and system (7). According to Eqs. (10)–(12), when $e(t) \to 0$, $\nabla_{\hat{A}} \omega(\hat{A}, \hat{B}, t) \to 0$, and $\nabla_{\hat{B}} \omega(\hat{A}, \hat{B}, t) \to 0$, therefore, \hat{A}, \hat{B} converge to real constant vectors. The proof is completed.

If A is a complex vector, then A can be written as $A = A^{r} + jA^{i}$. Therefore, equation (7) becomes

$$\dot{\boldsymbol{w}} = \boldsymbol{F}(\boldsymbol{w})\boldsymbol{A}^{\mathrm{r}} + \mathrm{j}\boldsymbol{F}(\boldsymbol{w})\boldsymbol{A}^{\mathrm{i}} + \boldsymbol{f}(\boldsymbol{w}) + \boldsymbol{v}$$

$$= \boldsymbol{F}(\boldsymbol{w})\boldsymbol{A}^{\mathrm{r}} + \boldsymbol{R}(\boldsymbol{w})\boldsymbol{A}^{\mathrm{l}} + \boldsymbol{f}(\boldsymbol{w}) + \boldsymbol{v}, \qquad (16)$$

where $\mathbf{R}(\mathbf{w}) = \mathbf{j}\mathbf{F}(\mathbf{w})$ is a new $n \times m$ complex matrix. Therefore, we have

Theorem 2 If the adaptive controller is designed as

$$v = -F(w)\hat{A}^{\mathrm{r}} - R(w)\hat{A}^{\mathrm{i}} - f(w) + HG(z)\hat{B}$$

+ $Hg(z) + Ke$
= $-F(w)^{\mathrm{r}}\hat{A}^{\mathrm{r}} - R(w)^{\mathrm{r}}\hat{A}^{\mathrm{i}} - f(w)^{\mathrm{r}} + H^{\mathrm{r}}G(z)\hat{B}$
+ $H^{\mathrm{r}}g(z) + Ke^{\mathrm{r}} + \mathrm{j}[-F(w)^{\mathrm{i}}\hat{A}^{\mathrm{r}} - R(w)^{\mathrm{i}}\hat{A}^{\mathrm{i}}$
- $f(w)^{\mathrm{i}} + H^{\mathrm{i}}G(z)\hat{B} + H^{\mathrm{i}}g(z) + Ke^{\mathrm{i}}],$ (17)

and the adaptive laws are selected as

$$\begin{cases} \hat{A}^{\mathrm{r}} = -\lambda \nabla_{\hat{A}^{\mathrm{r}}} \omega(\hat{A}^{\mathrm{r}}, \hat{A}^{\mathrm{i}}, \hat{B}, t) \\ &-\eta \int_{0}^{t} \nabla_{\hat{A}^{\mathrm{r}}} \omega(\hat{A}^{\mathrm{r}}, \hat{A}^{\mathrm{i}}, \hat{B}, \alpha) \mathrm{d}\alpha, \\ \hat{A}^{\mathrm{i}} = -\lambda' \nabla_{\hat{A}^{\mathrm{i}}} \omega(\hat{A}^{\mathrm{r}}, \hat{A}^{\mathrm{i}}, \hat{B}, \alpha) \mathrm{d}\alpha, \\ &-\eta' \int_{0}^{t} \nabla_{\hat{A}^{\mathrm{i}}} \omega(\hat{A}^{\mathrm{r}}, \hat{A}^{\mathrm{i}}, \hat{B}, \alpha) \mathrm{d}\alpha, \\ \hat{B} = -\varsigma \nabla_{\hat{B}} \omega(\hat{A}^{\mathrm{r}}, \hat{A}^{\mathrm{i}}, \hat{B}, \alpha) \mathrm{d}\alpha, \\ &-\tau \int_{0}^{t} \nabla_{\hat{B}} \omega(\hat{A}^{\mathrm{r}}, \hat{A}^{\mathrm{i}}, \hat{B}, \alpha) \mathrm{d}\alpha, \\ &\dot{k}_{l} = -\eta [e_{l}^{\mathrm{r}}(t)^{2} + e_{l}^{\mathrm{i}}(t)^{2}], \ l = 1, 2, \dots, n, \end{cases}$$
(18)

where

$$\nabla_{\hat{A}^{\mathrm{r}}} \boldsymbol{\omega}(\hat{A}^{\mathrm{r}}, \hat{A}^{\mathrm{i}}, \hat{B}, t) = -(\boldsymbol{F}^{\mathrm{T}}(\boldsymbol{w})^{\mathrm{r}}, \boldsymbol{F}^{\mathrm{T}}(\boldsymbol{w})^{\mathrm{i}}) \begin{bmatrix} \boldsymbol{e}^{\mathrm{r}} \\ \boldsymbol{e}^{\mathrm{i}} \end{bmatrix}, \qquad (19)$$
$$\nabla_{\hat{a}^{\mathrm{i}}} \boldsymbol{\omega}(\hat{A}^{\mathrm{r}}, \hat{A}^{\mathrm{i}}, \hat{B}, t)$$

$$= -(\boldsymbol{R}^{\mathrm{T}}(\boldsymbol{w})^{\mathrm{r}}, \boldsymbol{R}^{\mathrm{T}}(\boldsymbol{w})^{\mathrm{i}}) \begin{bmatrix} \boldsymbol{e}^{\mathrm{r}} \\ \boldsymbol{e}^{\mathrm{i}} \end{bmatrix}, \qquad (20)$$
$$\nabla_{\hat{\boldsymbol{x}}} \boldsymbol{\omega}(\hat{\boldsymbol{A}}^{\mathrm{r}}, \hat{\boldsymbol{A}}^{\mathrm{i}}, \hat{\boldsymbol{B}}, t)$$

$$= ((\boldsymbol{H}^{\mathrm{r}}\boldsymbol{G}(\boldsymbol{z}))^{\mathrm{T}}, (\boldsymbol{H}^{\mathrm{i}}\boldsymbol{G}(\boldsymbol{z}))^{\mathrm{T}}) \begin{bmatrix} \boldsymbol{e}^{\mathrm{r}} \\ \boldsymbol{e}^{\mathrm{i}} \end{bmatrix}, \qquad (21)$$

where $\lambda' = \text{diag}(\lambda'_1, \lambda'_2, ..., \lambda'_n)$ and $\eta' = \text{diag}(\eta'_1, \eta'_2, ..., \eta'_n)$ are corresponding convergence factor matrixes and their elements are positive real constants, then the response system (16) synchronizes the real drive chaotic system (6) in sense of CMPS asymptotically, and \hat{A}^r , \hat{A}^i , \hat{B} converge to real constant vectors.

Proof It is similar to the proof in Theorem 1 and thus is omitted.

4. CMPS schemes of complex drive chaotic system and real response chaotic system

4.1. Mathematical model and problem descriptions

In this section, we consider the following *n*-dimensional complex drive chaotic system with unknown parameters,

$$\dot{\boldsymbol{y}} = \boldsymbol{Q}(\boldsymbol{y})\boldsymbol{D} + \boldsymbol{q}(\boldsymbol{y}), \qquad (22)$$

where $y = (y_1, y_2, ..., y_n)^T$ is a complex state vector. Set $y_1 = u'_1 + ju'_2, y_2 = u'_3 + ju'_4, ..., y_n = u'_{2n-1} + ju'_{2n}$, and $y^r = u'_1 + ju'_2 + ju'_2$

 $(u'_1, u'_3, \ldots, u'_{2n-1})^T$, $y^i = (u'_2, u'_4, \ldots, u'_{2n})^T$. Q(y) is an $n \times s$ complex matrix and its elements are functions of complex state variables, $D = (d_1, d_2, \ldots, d_s)^T$ is an $s \times 1$ real (complex) vector of unknown parameters, and $q = (q_1, q_2, \ldots, q_n)^T$ is a vector of a complex nonlinear function.

The real response chaotic system is depicted as,

$$\dot{\boldsymbol{x}} = \boldsymbol{P}(\boldsymbol{x})\boldsymbol{C} + \boldsymbol{p}(\boldsymbol{x}) + \boldsymbol{L}, \qquad (23)$$

where $\boldsymbol{x} = (x_1, x_2, ..., x_n)^T$ is a real state vector. $\boldsymbol{P}(\boldsymbol{x})$ is an $n \times m$ real matrix, and $\boldsymbol{C} = (c_1, c_2, ..., c_m)^T$ is an $m \times 1$ real vector of unknown parameters, and $\boldsymbol{p} = (p_1, p_2, ..., p_n)^T$ is a vector of real nonlinear function. The designed controller is \boldsymbol{L} .

We first give the special definition of CMPS of complex drive chaotic systems and real response chaotic systems.

Definition 2 For the drive system (22) and response system (23), if there exists a complex constant matrix $H = \text{diag}\{h_1 + jh_2, h_3 + jh_4, \dots, h_{2n-1} + jh_{2n}\}$ such that

$$\lim_{t\to\infty} \|\boldsymbol{e}(t)\|^2 = \lim_{t\to\infty} \|\boldsymbol{x}(t) - \boldsymbol{H}^{\mathrm{r}}\boldsymbol{y}^{\mathrm{r}}(t) + \boldsymbol{H}^{\mathrm{i}}\boldsymbol{y}^{\mathrm{i}}(t)\|^2 = 0, \quad (24)$$

where $e(t) = x(t) - H^{r}y^{r}(t) + H^{i}y^{i}(t)$ is the real error vector, then the complex drive system (22) and real response system (23) are CMPS of real parts. As x(t) is real, we choose real L to ensure CMPS of real parts and avoid increasing the imaginary parts of response system. The control objective is to design an adaptive real controller L such that the response real system (23) can synchronize the drive complex system (22) asymptotically in sense of the CMPS of real parts.

4.2. Adaptive CMPS schemes of real parts

If *D* is a real vector, we have the following theorem. **Theorem 3** If the adaptive controller is designed as

$$L = -P(x)\hat{C} - p(x) + (H^{\mathrm{r}}Q(y)^{\mathrm{r}} - H^{\mathrm{l}}Q(y)^{\mathrm{l}})\hat{D} + H^{\mathrm{r}}q(y)^{\mathrm{r}} - H^{\mathrm{i}}q(y)^{\mathrm{i}} + Ke, \qquad (25)$$

where \hat{C} , \hat{D} are the estimated values of C and D, respectively; and the adaptive laws are selected as

$$\begin{cases} \hat{\boldsymbol{C}} = -\lambda \nabla_{\hat{\boldsymbol{C}}} \boldsymbol{\omega}(\hat{\boldsymbol{C}}, \hat{\boldsymbol{D}}, t) - \eta \int_{0}^{t} \nabla_{\hat{\boldsymbol{C}}} \boldsymbol{\omega}(\hat{\boldsymbol{C}}, \hat{\boldsymbol{D}}, \alpha) \, \mathrm{d}\alpha, \\ \hat{\boldsymbol{D}} = -\varsigma \nabla_{\hat{\boldsymbol{D}}} \boldsymbol{\omega}(\hat{\boldsymbol{C}}, \hat{\boldsymbol{D}}, t) - \boldsymbol{\tau} \int_{0}^{t} \nabla_{\hat{\boldsymbol{D}}} \boldsymbol{\omega}(\hat{\boldsymbol{C}}, \hat{\boldsymbol{D}}, \alpha) \, \mathrm{d}\alpha, \quad (26) \\ \dot{\boldsymbol{k}}_{l} = -\gamma_{l} [\boldsymbol{e}_{l}^{\mathrm{r}}(t)^{2} + \boldsymbol{e}_{l}^{\mathrm{i}}(t)^{2}], \quad l = 1, 2, \cdots, n, \end{cases}$$

where

$$\nabla_{\hat{\boldsymbol{C}}}\boldsymbol{\omega}(\hat{\boldsymbol{C}},\hat{\boldsymbol{D}},t) = -\boldsymbol{P}^{\mathrm{T}}(\boldsymbol{x})\boldsymbol{e},\tag{27}$$

$$\nabla_{\hat{\boldsymbol{D}}}\boldsymbol{\omega}(\hat{\boldsymbol{C}},\hat{\boldsymbol{D}},t) = (\boldsymbol{H}^{\mathrm{r}}\boldsymbol{Q}(\boldsymbol{y})^{\mathrm{r}} - \boldsymbol{H}^{\mathrm{i}}\boldsymbol{Q}(\boldsymbol{y})^{\mathrm{i}})^{\mathrm{T}}\boldsymbol{e}, \quad (28)$$

then the response system (23) and the drive chaotic system (22) will be CMPS for real parts and \hat{C} , \hat{D} converge to real constant vectors.

Proof It is similar to the proof in Theorem 1 and thus is omitted.

If D is a complex vector, then D can be written as $D = D^{r} + jD^{i}$ and expression (22) becomes

$$\dot{\boldsymbol{y}} = \boldsymbol{Q}(\boldsymbol{y})\boldsymbol{D}^{\mathrm{r}} + \mathrm{j}\boldsymbol{Q}(\boldsymbol{y})\boldsymbol{D}^{\mathrm{l}} + \boldsymbol{q}(\boldsymbol{y})$$

$$= \boldsymbol{Q}(\boldsymbol{y})\boldsymbol{D}^{\mathrm{r}} + \boldsymbol{O}(\boldsymbol{y})\boldsymbol{D}^{\mathrm{l}} + \boldsymbol{q}(\boldsymbol{y}),$$
(29)

where O(y) = jQ(y) is a new $n \times m$ complex matrix. Therefore, we have the following theorem.

Theorem 4 If the adaptive controller is designed as

$$L = -P(x)\hat{C} - p(x) + (H^{\mathrm{r}}Q(y)^{\mathrm{r}} - H^{\mathrm{l}}Q(y)^{\mathrm{l}})\hat{D}^{\mathrm{r}} + (H^{\mathrm{r}}O(y)^{\mathrm{r}} - H^{\mathrm{i}}O(y)^{\mathrm{i}})\hat{D}^{\mathrm{i}} + H^{\mathrm{r}}q(y)^{\mathrm{r}} - H^{\mathrm{i}}q(y)^{\mathrm{i}} + Ke$$
(30)

and the adaptive laws are selected as

$$\begin{cases} \hat{C} = -\lambda \nabla_{\hat{C}} \omega(\hat{C}, \hat{D}^{\mathrm{r}}, \hat{D}^{\mathrm{i}}, t) \\ &-\eta \int_{0}^{t} \nabla_{\hat{C}} \omega(\hat{C}, \hat{D}^{\mathrm{r}}, \hat{D}^{\mathrm{i}}, \alpha) \mathrm{d}\alpha, \\ \hat{D}^{\mathrm{r}} = -\varsigma \nabla_{\hat{D}^{\mathrm{r}}} \omega(\hat{C}, \hat{D}^{\mathrm{r}}, \hat{D}^{\mathrm{i}}, \alpha) \mathrm{d}\alpha, \\ &-\tau \int_{0}^{t} \nabla_{\hat{D}^{\mathrm{r}}} \omega(\hat{C}, \hat{D}^{\mathrm{r}}, \hat{D}^{\mathrm{i}}, \alpha) \mathrm{d}\alpha, \\ \hat{D}^{\mathrm{i}} = -\varsigma' \nabla_{\hat{D}^{\mathrm{i}}} \omega(\hat{C}, \hat{D}^{\mathrm{r}}, \hat{D}^{\mathrm{i}}, \alpha) \mathrm{d}\alpha, \\ &\hat{D}^{\mathrm{i}} = -\gamma' \int_{0}^{t} \nabla_{\hat{D}^{\mathrm{i}}} \omega(\hat{C}, \hat{D}^{\mathrm{r}}, \hat{D}^{\mathrm{i}}, \alpha) \mathrm{d}\alpha, \\ &k_{l} = -\gamma_{l} [e_{l}^{\mathrm{r}}(t)^{2} + e_{l}^{\mathrm{i}}(t)^{2}], \ l = 1, 2, \dots, n, \end{cases}$$
(31)

where

$$\nabla_{\hat{\boldsymbol{C}}}\boldsymbol{\omega}(\hat{\boldsymbol{C}}, \hat{\boldsymbol{D}}^{\mathrm{r}}, \hat{\boldsymbol{D}}^{\mathrm{i}}, t) = -\boldsymbol{P}^{\mathrm{T}}(\boldsymbol{x})\boldsymbol{e}, \qquad (32)$$

$$\nabla_{\hat{\boldsymbol{D}}^{\mathrm{r}}}\boldsymbol{\omega}(\hat{\boldsymbol{C}},\hat{\boldsymbol{D}}^{\mathrm{r}},\hat{\boldsymbol{D}}^{\mathrm{i}},t) = (\boldsymbol{H}^{\mathrm{r}}\boldsymbol{Q}(\boldsymbol{y})^{\mathrm{r}} - \boldsymbol{H}^{\mathrm{i}}\boldsymbol{Q}(\boldsymbol{y})^{\mathrm{i}})^{\mathrm{T}}\boldsymbol{e}, \quad (33)$$

$$\nabla_{\hat{\boldsymbol{D}}^{i}}\boldsymbol{\omega}(\hat{\boldsymbol{C}},\hat{\boldsymbol{D}}^{r},\hat{\boldsymbol{D}}^{i},t) = (\boldsymbol{H}^{r}\boldsymbol{O}(\boldsymbol{y})^{r} - \boldsymbol{H}^{i}\boldsymbol{O}(\boldsymbol{y})^{i})^{T}\boldsymbol{e},\quad(34)$$

where $\varsigma' = \text{diag}(\varsigma'_1, \varsigma'_2, ..., \varsigma'_n)$ and $\tau' = \text{diag}(\tau'_1, \tau'_2, ..., \tau'_n)$ are the convergence factor matrix and its elements are positive real constants, then the response system (23) and the drive chaotic system (29) will be CMPS for real parts, and \hat{C} , \hat{D}^r , \hat{D}^i converge to real constant vectors.

Proof It is similar to the proof in Theorem 1 and thus is omitted.

Obviously, the CMPS of imaginary parts is similar to the CMPS of real parts, and thus is omitted.

5. Simulations

5.1. CMPS of real hyperchaotic Rössler system and complex hyperchaotic Lorenz system

In order to observe CMPS behaviors of the real drive system and complex response system, we assume that the real hyperchaotic Rössler system^[27] drives the complex hyperchaotic Lorenz system.^[28] The drive hyperchaotic Rössler system is defined as follows:

$$\begin{cases} \dot{z}_1 = -z_2 - z_3, \\ \dot{z}_2 = z_1 + b_1 z_2 + z_4, \\ \dot{z}_3 = b_2 + z_1 z_3, \\ \dot{z}_4 = -b_3 z_3 + b_4 z_4, \end{cases}$$
(35)

where

$$oldsymbol{G}(oldsymbol{z}) = egin{pmatrix} 0 & 0 & 0 & 0 \ z_2 & 0 & 0 & 0 \ 0 & 1 & 0 & 0 \ 0 & 0 & -z_3 & z_4 \end{pmatrix}, \ oldsymbol{g}(oldsymbol{z}) = egin{pmatrix} -z_2 - z_3 \ z_1 + z_4 \ z_1 z_3 \ 0 \ \end{pmatrix},$$

and z_1 , z_2 , z_3 , and z_4 are real state variables, B = $(b_1, b_2, b_3, b_4)^{\mathrm{T}}$ is the unknown parameter vector.

The complex response hyperchaotic Lorenz system is

$$\begin{cases} \dot{w}_1 = a_1(w_2 - w_1), \\ \dot{w}_2 = a_2w_1 - w_2 - w_1w_3 + w_4, \\ \dot{w}_3 = -a_3w_3 + (1/2)(\bar{w}_1w_2 + w_1\bar{w}_2), \\ \dot{w}_4 = a_4w_1 + a_5w_2, \end{cases}$$
(36)

where

$$\boldsymbol{F}(\boldsymbol{w}) = \begin{pmatrix} w_2 - w_1 & 0 & 0 & 0 & 0 \\ 0 & w_1 & 0 & 0 & 0 \\ 0 & 0 & -w_3 & 0 & 0 \\ 0 & 0 & 0 & w_1 & w_2 \end{pmatrix},$$
$$\boldsymbol{f}(\boldsymbol{w}) = \begin{pmatrix} 0 \\ -w_2 - w_1 w_3 + w_4 \\ (1/2)(\bar{w}_1 w_2 + w_1 \bar{w}_2) \\ 0 \end{pmatrix},$$

where $w_1 = u_1 + ju_2$, $w_2 = u_3 + ju_4$, $w_4 = u_6 + ju_7$ are complex state variables and $w_3 = u_5$ is a real state variable, a_1, a_2, a_3, a_4, a_5 are real unknown parameters. The overbar $\bar{w}_1(\bar{w}_2)$ stands for the complex conjugate of $w_1(w_2)$.

We design the controller according to Theorem 1 as follows:

$$\begin{split} \mathbf{v} &= -\mathbf{F}(\mathbf{w})\hat{\mathbf{A}} - \mathbf{f}(\mathbf{w}) + \mathbf{H}\mathbf{G}(\mathbf{z})\hat{\mathbf{B}} + \mathbf{H}\mathbf{g}(\mathbf{z}) + \mathbf{K}\mathbf{e} \\ &= \begin{pmatrix} -\hat{a}_{1}(w_{2} - w_{1}) + (h_{1} + \mathbf{j}h_{2})(-z_{2} - z_{3}) + k_{1}(e_{1} + \mathbf{j}e_{2}) \\ -\hat{a}_{2}w_{1} + w_{2} + w_{1}w_{3} - w_{4} + (h_{3} + \mathbf{j}h_{4})(z_{1} + \hat{b}_{1}z_{2} + z_{4}) + k_{2}(e_{3} + \mathbf{j}e_{4}) \\ \hat{a}_{3}w_{3} - (1/2)(\bar{w}_{1}w_{2} + w_{1}\bar{w}_{2}) + h_{5}(\hat{b}_{2} + z_{1}z_{3}) + k_{3}e_{5} \\ -\hat{a}_{4}w_{1} - \hat{a}_{5}w_{2} + (h_{6} + \mathbf{j}h_{7})(-\hat{b}_{3}z_{3} + \hat{b}_{4}z_{4}) + k_{4}(e_{6} + \mathbf{j}e_{7}) \end{pmatrix} \\ &= \begin{pmatrix} -\hat{a}_{1}(u_{3} - u_{1}) + h_{1}(-z_{2} - z_{3}) + k_{1}e_{1} \\ -\hat{a}_{2}u_{1} + u_{3} + u_{1}u_{5} - u_{6} + h_{3}(z_{1} + \hat{b}_{1}z_{2} + z_{4}) + k_{2}e_{3} \\ \hat{a}_{3}u_{5} - (u_{1}u_{3} + u_{2}u_{4}) + h_{5}(\hat{b}_{2} + z_{1}z_{3}) + k_{3}e_{5} \\ -\hat{a}_{4}u_{1} - \hat{a}_{5}u_{3} + h_{6}(-\hat{b}_{3}z_{3} + \hat{b}_{4}z_{4}) + k_{4}e_{6} \end{pmatrix} + \mathbf{j} \begin{pmatrix} -\hat{a}_{1}(u_{4} - u_{2}) + h_{2}(-z_{2} - z_{3}) + k_{1}e_{2} \\ -\hat{a}_{2}u_{2} + u_{4} + u_{2}u_{5} - u_{7} + h_{4}(z_{1} + \hat{b}_{1}z_{2} + z_{4}) + k_{2}e_{4} \\ 0 \\ -\hat{a}_{4}u_{2} - \hat{a}_{5}u_{4} + h_{7}(-\hat{b}_{3}z_{3} + \hat{b}_{4}z_{4}) + k_{4}e_{7} \end{pmatrix} \end{split}$$

where $h_1 + jh_2$, $h_3 + jh_4$, h_5 , $h_6 + jh_7$ are scaling factors, $e_1 = u_1 - h_1 z_1, e_2 = u_2 - h_2 z_1, e_3 = u_3 - h_3 z_2, e_4 = u_4 - h_4 z_2,$ $e_5 = u_5 - h_5 z_3$, $e_6 = u_6 - h_6 z_4$, and $e_7 = u_7 - h_7 z_4$.

The adaptive laws are taken as Eq. (10), where

$$\nabla_{\hat{A}}\omega(\hat{A},\hat{B},t) = \begin{pmatrix} -[(u_3 - u_1)e_1 + (u_4 - u_2)e_2] \\ -[u_1e_3 + u_2e_4] \\ u_5e_5 \\ -(u_1e_6 + u_2e_7) \\ -(u_3e_6 + u_4e_7) \end{pmatrix}, \quad (38)$$

$$\nabla_{\hat{B}}\omega(\hat{A},\hat{B},t) = \begin{pmatrix} h_3z_2e_3 + h_4z_2e_4 \\ h_5e_5 \\ -h_6z_3e_6 - h_7z_3e_7 \\ h_6z_4e_6 + h_7z_4e_7 \end{pmatrix}, \quad (39)$$

and

$$\dot{\boldsymbol{k}} = \begin{pmatrix} \dot{k}_1 \\ \dot{k}_2 \\ \dot{k}_3 \\ \dot{k}_4 \end{pmatrix} = \begin{pmatrix} -\gamma_1(e_1^2 + e_2^2) \\ -\gamma_2(e_3^2 + e_4^2) \\ -\gamma_3e_5^2 \\ -\gamma_4(e_6^2 + e_7^2) \end{pmatrix}.$$
 (40)

The true values of unknown parameters are A = $(14,35,3,-5,-4)^{\mathrm{T}}$ and $\boldsymbol{B} = (0.25,3,0.5,0.05)^{\mathrm{T}}$. The initial conditions of the drive system (35) and the response system (36) are $z(0) = (-20, 0, 0, 15)^{T}$ and w(0) =

$$\begin{pmatrix} -\hat{a}_{1}(u_{4}-u_{2})+h_{2}(-z_{2}-z_{3})+k_{1}e_{2}\\ -\hat{a}_{2}u_{2}+u_{4}+u_{2}u_{5}-u_{7}+h_{4}(z_{1}+\hat{b}_{1}z_{2}+z_{4})+k_{2}e_{4}\\ 0\\ -\hat{a}_{4}u_{2}-\hat{a}_{5}u_{4}+h_{7}(-\hat{b}_{3}z_{3}+\hat{b}_{4}z_{4})+k_{4}e_{7} \end{pmatrix},$$
(37)

 $(-1 - 2j, -3 - 4j, -5, -6 - 7j)^{\mathrm{T}}$. The initial values of estimated parameters and control strength are $\hat{A}(0) =$ $(10, 10, 10, 10, 10)^{\mathrm{T}}, \hat{B}(0) = (1, 1, 1, 1)^{\mathrm{T}}, \text{ and } k(0) =$ $(0, 0, 0, 0)^{T}$. The fourth-order Runge-Kutta scheme is utilized to solve the differential equations with $\Delta t = 10^{-3}$ s. The CMPS process of systems (35) and (36) is shown in Fig. 1, where the solid line shows the states of the drive system and the dotted line presents the states of the response system. Their chaotic behaviors are shown in Figs. 2 and 3, where the red line shows the trajectory of the drive system and the blue line presents the trajectory of the response system. The real parts $(w_1^{\rm r}, w_2^{\rm r}, w_3)$ of the response system (36) completely synchronize (z_1, z_2, z_3) of the drive system (35) in Fig. 2 as $h_1 = h_3 = h_5 = 1$, while the imaginary parts (w_1^i, w_2^i, w_4^i) of the response system (36) anti-synchronize (z_1, z_2, z_4) of the drive system (35) in Fig. 3 as $h_2 = h_4 = h_7 = -1$. The errors of CMPS converge asymptotically to zero as demonstrated in Fig. 4.

The processes of parameters identification of \hat{A} and \hat{B} are shown in Figs. 5 and 6 respectively. The estimated vector \hat{A} converges to

$$(14.0383, 34.9475, 2.9451, -5.0000, -4.0000)^{\mathrm{T}}$$

while \hat{B} converges to $(0.2071, 3.0332, 0.5231, 0.0523)^{T}$, which are near the true value.

5.2. CMPS of complex Lorenz drive system and real Lorenz response system

In order to observe CMPS behaviors of the complex drive system and the real response system, we assume that the uncertain complex Lorenz system drives the uncertain real Lorenz system. Therefore, the complex drive system is defined as follows:

$$\begin{cases} \dot{y}_1 = d_1(y_2 - y_1), \\ \dot{y}_2 = d_2 y_1 - y_1 y_3 - y_2, \\ \dot{y}_3 = -d_3 y_3 + (1/2)(\bar{y}_1 y_2 + y_1 \bar{y}_2), \end{cases}$$
(41)



Fig. 1. (color online) The CMPS of systems (35) and (36) with $\eta_1 = 0.05$, $\eta_2 = \eta_3 = 1$, $\eta_4 = \eta_5 = 0.1$, $\lambda_1 = \lambda_2 = \lambda_3 = \lambda_4 = \lambda_5 = 0.01$, $\zeta_1 = \zeta_2 = \zeta_3 = \zeta_4 = 0.01$, $\tau_1 = 0.05$, $\tau_2 = \tau_3 = 1$, $\tau_4 = 0.1$, $\gamma_1 = \gamma_2 = \gamma_3 = \gamma_4 = 10$ and complex scaling factors 1 - j, 1 - j, 1, 1 - j. Panel (a) [(a1)–(a4)]: The CMPS of state variables w_1 , z_1 and w_2 , z_2 . Panel (b) [(b1)–(b3)]: The CMPS of state variables w_3 , z_3 and w_4 , z_4 .



Fig. 2. (color online) The real parts (w_1^r, w_2^r, w_3) of system (36) synchronize (z_1, z_2, z_3) of system (35) as $h_1 = h_3 = h_5 = 1$.



Fig. 3. (color online) The imaginary parts (w_1^i, w_2^i, w_4^i) of system (36) anti-synchronize (z_1, z_2, z_4) of system (35) as $h_2 = h_4 = h_7 = -1$.



Fig. 4. (color online) The error dynamic of CMPS of systems (35) and (36). Panel (a) [(a1)-(a4)]: The error between complex state variables x_1 , $(1 - j)z_1$ and w_2 , $(1 - j)z_2$. Panel (b) [(b1)–(b3)]: The error between complex state variables x_3 , z_3 , and x_4 , $(1 - j)z_4$.



Fig. 5. (color online) The identification process of unknown parameter vector A.



Fig. 6. (color online) The identification process of unknown parameter vector B.

where

$$Q(y) = \begin{pmatrix} y_2 - y_1 & 0 & 0 \\ 0 & y_1 & 0 \\ 0 & 0 & -y_3 \end{pmatrix},$$

$$q(y) = \begin{pmatrix} 0 \\ -y_1y_3 - y_2 \\ (1/2)(\bar{y}_1y_2 + y_1\bar{y}_2) \end{pmatrix},$$

$$-ju'_2 \text{ and } y_2 = u'_3 + ju'_4 \text{ are complex state varieus}, D = (d_1, d_2, d_3)^{\mathrm{T}} \text{ is}$$

$$P(x) = \begin{pmatrix} x_2 - x_1 & 0 & 0 \\ 0 & x_1 & 0 \\ 0 & 0 & -x_3 \end{pmatrix}, p(x) = \begin{pmatrix} 0 \\ -x_2 - x_1x_3 \\ x_1x_2 \end{pmatrix},$$

$$(42)$$

 $\boldsymbol{P}(\boldsymbol{x}) =$

and $y_1 = u'_1 + ju'_2$ and $y_2 = u'_3 + ju'_4$ are complex state variables, and $y_3 = u'_5$ is a real state variable, $D = (d_1, d_2, d_3)^T$ is the unknown parameter vector.

where x_1, x_2, x_3 are real state variables, and c_1, c_2, c_3 are real unknown parameters.

We design the controller according to Theorem 3 as follows:

$$v = -P(x)\hat{C} - p(x) + (H^{r}Q(y)^{r} - H^{i}Q(y)^{i})\hat{D} + H^{r}q(y)^{r} - Hq(y)^{i} + Ke$$

$$= \begin{pmatrix} -\hat{c}_{1}(x_{2} - x_{1}) + [h_{1}(u'_{3} - u'_{1}) - h_{2}(u'_{4} - u'_{2})]\hat{d}_{1} + k_{1}e_{1} \\ -\hat{c}_{2}x_{1} + x_{2} + x_{1}x_{3} + (h_{3}u'_{1} - h_{4}u'_{2})\hat{d}_{2} - h_{3}(u'_{1}u'_{5} + u'_{3}) + h_{4}(u'_{2}u'_{5} + u'_{4}) + k_{2}e_{2} \\ \hat{c}_{3}x_{3} - x_{1}x_{2} + h_{5}(-\hat{d}_{3}u'_{5} + u'_{1}u'_{3} + u'_{2}u'_{4}) + k_{3}e_{3} \end{pmatrix},$$
(43)

where $h_1 + jh_2$, $h_3 + jh_4$, h_5 are scaling factors, $e_1 = x_1 - (h_1u'_1 - h_2u'_2)$, $e_2 = x_2 - (h_3u'_3 - h_4u'_4)$, and $e_3 = x_3 - h_5u'_5$.

The adaptive laws are taken as expression (26) where

$$\nabla_{\hat{C}}\omega(\hat{C},\hat{D},t) = \begin{pmatrix} -(x_2 - x_1)e_1 \\ -x_1e_2 \\ x_3e_3 \end{pmatrix},$$
 (44)

$$\nabla_{\hat{\boldsymbol{D}}}\boldsymbol{\omega}(\hat{\boldsymbol{C}},\hat{\boldsymbol{D}},t) = \begin{pmatrix} e_1[h_1(u_3' - u_1') - h_2(u_4' - u_2')] \\ e_2(h_3u_1' - h_4u_2') \\ -u_5'e_5 \end{pmatrix}, \quad (45)$$

and

$$\dot{\boldsymbol{k}} = \begin{pmatrix} \dot{k}_1 \\ \dot{k}_2 \\ \dot{k}_3 \end{pmatrix} = \begin{pmatrix} -\gamma_1 e_1^2 \\ -\gamma_2 e_2^2 \\ -\gamma_3 e_3^2 \end{pmatrix}.$$
(46)

The true values of unknown parameters are C = $(10, 28, 8/3)^{T}$ and $D = (35, 55, 8/3)^{T}$. The initial conditions are $y(0) = (-1 - 2i, -3 - 4i, -5)^{T}$ and x(0) = $(-1, -3, -5)^{T}$. The initial values of estimated parameters and control strength are $\hat{C}(0) = (20, 20, 20)^{\mathrm{T}}, \hat{D}(0) =$ $(10, 10, 10)^{T}$, and $k(0) = (0, 0, 0)^{T}$. The fourth-order Runge-Kutta scheme is utilized to solve the differential equations with $\Delta t = 10^{-3}$ s. The CMPS process of systems (41) and (42) is shown in Fig. 7, where the solid line shows the states of the drive system and the dotted line presents the states of the response system. Their chaotic behaviors are shown in Fig. 8, where the red line shows the trajectory of the drive system and the blue line presents the trajectory of the response system. The response system (42) synchronizes the real parts of the product of H and complex drive system (41) in Fig. 8. The errors of CMPS converge asymptotically to zero as demonstrated in Fig. 9. The processes of parameters identification of \hat{C} and \hat{D} are shown in Fig. 10. Obviously, the estimated values of \hat{C} and \hat{D} converge to certain constants.



Fig. 7. (color online) The CMPS of systems (41) and (42) with $\eta_1 = \eta_2 = \eta_3 = 1$, $\lambda_1 = \lambda_2 = \lambda_3 = 0.01$, $\zeta_1 = \zeta_2 = \zeta_3 = 0.01$, $\tau_1 = \tau_2 = \tau_3 = 1$, $\gamma_1 = \gamma_2 = \gamma_3 = 1$, and complex scaling factors -2 + j, -2 + j, -2.



Fig. 8. (color online) The response system (42) synchronizes the real parts $(-2y_1^r - y_1^i, -2y_2^r - y_2^i, -2y_3)$ of the product that the drive system (41) multiplied by complex scaling factors -2+j, -2+j, -2.







Fig. 10. (color online) The identification process of unknown parameter vectors C and D.

6. Conclusion

We give the definition of CMPS of complex chaotic systems and real chaotic systems and design corresponding adaptive CMPS schemes considering all situations of unknown parameters and pseudo-gradient condition based on the SG method. The convergence factors and the dynamical control strength are added to regulate the convergence speed and increase the robustness of the uncertain response system, which is significant in practical applications. The theoretical result is verified by numerical examples, and the simulations demonstrate the effectiveness of the proposed synchronization scheme.

Moreover, the CMPS establishes a link between real chaotic systems and complex chaotic systems, which increases the complexity and scope of the synchronization and directs high security and large variety of secure communications.

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Chinese Physics B

Volume 22 Number 12 December 2013

	TOPICAL REVIEW — Magnetism, magnetic materials, and interdisciplinary research		
127301	Tuning the electrons at the LaAlO ₃ /SrTiO ₃ interface: From growth to beyond growth		
	Xie Yan-Wu and Hwang Harold Y		
127502	Fabrication, properties, and applications of flexible magnetic films		
	Liu Yi-Wei, Zhan Qing-Feng and Li Run-Wei		
127503	Toxicity of superparamagnetic iron oxide nanoparticles: Research strategies and implications for		
	nanomedicine		
	Li Lei, Jiang Ling-Ling, Zeng Yun and Liu Gang		
	GENERAL		
120201	The periodic oscillations in the ENSO recharge–discharge oscillator model		
	Zhang Wu-Fan and Zhao Qiang		
120202	2 A self-adaptive stochastic resonance system design and study in chaotic interference		
	Lu Kang, Wang Fu-Zhong, Zhang Guang-Lu and Fu Wei-Hong		
120203	An improved interpolating element-free Galerkin method for elasticity		
	Sun Feng-Xin, Wang Ju-Feng and Cheng Yu-Min		
120204	A meshless model for transient heat conduction analyses of 3D axisymmetric functionally graded solids		
	Li Qing-Hua, Chen Shen-Shen and Zeng Ji-Hui		
120205	${ m GGA}$ + U study of the electronic energy bands and state density of the wurtzite ${ m In}_{1-x}{ m Ga}_x{ m N}$		
	Wang Wei-Hua, Zhao Guo-Zhong and Liang Xi-Xia		
120206	6 Simulating train movement in an urban railway based on an improved car-following model Ye Jing-Jing, Li Ke-Ping and Jin Xin-Min		
120301	New approach to $Q - P (P - Q)$ ordering of quantum mechanical operators and its applications		
	Hu Li-Yun, Zhang Hao-Liang, Jia Fang and Tao Xiang-Yang		
120302	Spin and pseudospin symmetries of the Dirac equation with shifted Hulthén potential using supersym-		
	metric quantum mechanics		
	Akpan N. Ikot, Elham Maghsoodi, Eno J. Ibanga, Saber Zarrinkamar and Hassan Hassanabadi		
120303	The squeezing dynamics of two independent atoms by detuning in two non-Markovian environments		
	Zou Hong-Mei, Fang Mao-Fa and Yang Bai-Yuan		
120304	The dynamics of three coupled dipolar Bose–Einstein condensates		
	Wu Jian-Hua and Xu Sheng-Nan		
120401	Conserved charges of Kerr-Ads spacetime using Poincaré gauge version		
	Gamal G. L. Nashed		

- 120402 High-frequency gravitational waves having large spectral densities and their electromagnetic response Li Fang-Yu, Wen Hao and Fang Zhen-Yun
- 120501 Scheduling of high-speed rail traffic based on discrete-time movement model Sun Ya-Hua, Cao Cheng-Xuan, Xu Yan and Wu Chao
- 120502 Codimension-two bifurcation of axial loaded beam bridge subjected to an infinite series of moving loads Yang Xin-Wei, Tian Rui-Lan and Li Hai-Tao
- 120503 Control of the patterns by using time-delayed feedback near the codimension-three Turing–Hopf–Wave bifurcations

Wang Hui-Juan, Wang Yong-Jie and Ren Zhi

120504 Effects of switching frequency and leakage inductance on slow-scale stability in a voltage controlled flyback converter

Wang Fa-Qiang and Ma Xi-Kui

120505 Modified projective synchronization with complex scaling factors of uncertain real chaos and complex chaos

Zhang Fang-Fang, Liu Shu-Tang and Yu Wei-Yong

- 120506 Stability of operation versus temperature of a three-phase clock-driven chaotic circuit Zhou Ji-Chao, Hyunsik Son, Namtae Kim and Han Jung Song
- 120507 Dynamic magnetic behavior of the mixed spin (2, 5/2) Ising system with antiferromagnetic/antiferromagnetic interactions on a bilayer square lattice

Mehmet Ertaş and Mustafa Keskin

120508 The Korteweg-de Vires equation for the bidirectional pedestrian flow model considering the nextnearest-neighbor effect

Xu Li, Lo Siu-Ming and Ge Hong-Xia

120701 Magnetic transition of ferromagnetic material at high pressure using a novel system

- 120702
- 120703

123101

- 123102
- 123103

Li Rui, Wei Chang-Li, Sun Qi-Xiang, Sun Er-Ping, Jin Ming-Xing, Xu Hai-Feng and Yan Bing

- 123201 Relativistic *R*-matrix studies of photoionization processes of Ar⁵⁺ Li Chuan-Yin, Han Xiao-Ying, Wang Jian-Guo and Qu Yi-Zhi
- 123401 Potential energy curve study on the ${}^{3}\Pi$ electronic states of GaX (X = F, Cl, and Br) molecules Cao Yun-Bin, Yang Chuan-Lu, Wang Mei-Shan and Ma Xiao-Guang
- 123402 Investigation of energy transfer from pyrromethene dye to cresyl violet 670 in ethanol Li Xiao-Hui, Fan Rong-Wei, Yu Xin and Chen De-Ying
- Structures, stabilities, and electronic properties of F-doped Si $_n$ $(n = 1 \sim 12)$ clusters: Density functional 123601 theory investigation

Zhang Shuai, Jiang Hua-Long, Wang Ping, Lu Cheng, Li Gen-Quan and Zhang Ping

123602 Computer study of the spectral characteristics of the disperse water-methane system A. Y. Galashev

ELECTROMAGNETISM, OPTICS, ACOUSTICS, HEAT TRANSFER, CLASSICAL MECHANICS, AND FLUID DYNAMICS

124101 Effects of self-fields on dispersion relation and growth rate in two-stream electromagnetically pumped free electron laser with axial guide magnetic field

S. Saviz and H. Rajabalinia

124102 Effects of density profile and multi-species target on laser-heated thermal-pressure-driven shock wave acceleration

Wang Feng-Chao

124201 Controlling the photoluminescence spectroscopy of quinacrine dihydrochloride by SiO₂ inverse opal photonic crystal

Li Chao-Rong, Yang Zhao-Ting, Xu Qing and Dong Wen-Jun

124202 A planar chiral nanostructure with asymmetric transmission of linearly polarized wave and huge optical activity in near-infrared band

Control of gain and thermal carrier loss profiles for mode optimization in 980-nm broad-area vertical-cavity surface-emitting lasers 124203

Wu Jian, Cui Huai-Yang, Huang Meng and Ma Ming-Lei

Mid-IR dual-wavelength difference frequency generation in uniform grating PPLN using index disper 124204 Chang Jian-Hua, Sun Qing, Ge Yi-Xian, Wang Ting-Ting, Tao Zai-Hong and Zhang Chuang

124205 A sensitive method of determining optic axis azimuth based on laser feedback

Wu Yun, Zhang Peng, Chen Wen-Xue and Tan Yi-Dong

Investigation of stimulated rotational Raman scattering of the high-power broadband laser with applied 124206 angular dispersion

Fan Xin-Min, Lü Zhi-Wei, Lin Dian-Yang, Liu Ying, Zhu Cheng-Yu, He Wei-Ming and Ding Lei

- 124207 Resisting shrinkage properties of volume holograms recorded in TiO₂ nanoparticle-dispersed acrylamide-based photopolymer Zhao Lei, Han Jun-He, Li Ruo-Ping, Wang Long-Ge and Huang Ming-Ju
- 124208 Polarization readout analysis for multilevel phase change recording by crystallization degree modulation Lin Jin-Cheng, Long Guo-Yun, Wang Yang and Wu Yi-Qun
- 124209 Efficient evanescent coupling design for GeSi electro-absorption modulator Li Ya-Ming and Cheng Bu-Wen
- 124301 Investigation of long-range sound propagation in surface ducts Duan Rui, Yang Kun-De and Ma Yuan-Liang
- 124601 Numerical analysis of the resonance mechanism of the lumped parameter system model for acoustic mine detection

Wang Chi, Zhou Yu-Qiu, Shen Gao-Wei, Wu Wen-Wen and Ding Wei

- 124701 Effects of transpiration on unsteady MHD flow of an upper convected Maxwell (UCM) fluid passing through a stretching surface in the presence of a first order chemical reaction Swati Mukhopadhyay, M. Golam Arif and M. Wazed Ali Pk
- 124702 Simultaneous effects of magnetic field and space porosity on compressible Maxwell fluid transport induced by a surface acoustic wave in a microchannel Khaled S. Mekheimer, Soliman R. Komy and Sara I. Abdelsalam
- 124703 Modelling the unsteady melt flow under a pulsed magnetic field Chen Guo-Jun, Zhang Yong-Jie and Yang Yuan-Sheng

PHYSICS OF GASES, PLASMAS, AND ELECTRIC DISCHARGES

125201 Investigation of impurity transport using supersonic molecular beam injected neon in HL-2A ECRH plasma

сонд тип-во, Gao Jin-Ming, Song Shao-Dong and Yang Qing-Wei Determinations of plasma density and decay time in the hollow cathode discharge by microwave trans-mission Zhang Lin, He Feng, Li Shi-Chao and Ouyang Ji-Ting CONDENSED MATTER: STRUCTURAL, MECHANICAL, AND THERMAL PROPERTIES 125202

- 126101 Chen Liang, Wang Tie-Shan, Zhang Gen-Fa, Yang Kun-Jie, Peng Hai-Bo and Zhang Li-Min
- 126102 A novel method to prepare Au nanocage@SiO₂ nanoparticle Jiang Tong-Tong, Yin Nai-Qiang, Liu Ling, Lei Jie-Mei, Zhu Li-Xin and Xu Xiao-Liang
- Effects of Cu on the martensitic transformation and magnetic properties of Mn₅₀Ni₄₀In₁₀ alloy 126201 Li Ge-Tian, Liu Zhu-Hong, Meng Fan-Yan, Ma Xing-Qiao and Wu Guang-Heng

126301 Investigations of high-pressure and high-temperature behaviors of the newly-discovered willemite-II and post-phenacite silicon nitrides

Chen Dong

- 126601 Molecular dynamics study of thermal stress and heat propagation in tungsten under thermal shock Fu Bao-Qin, Lai Wen-Sheng, Yuan Yue, Xu Hai-Yan, Li Chun, Jia Yu-Zhen and Liu Wei
- 126801 Expressions of the radius and the surface tension of surface of tension in terms of the pressure distribution for nanoscale liquid threads

Yan Hong, Wei Jiu-An, Cui Shu-Wen and Zhu Ru-Zeng

- 126802 Tensile properties of phase interfaces in Mg–Li alloy: A first principles study Zhang Cai-Li, Han Pei-De, Wang Xiao-Hong, Zhang Zhu-Xia, Wang Li-Ping and Xu Hui-Xia
- 126803 Pits and adatoms at the interface of 1-ML C₈₄/Ag (111) Wang Peng, Zhang Han-Jie, Li Yan-Jun, Sheng Chun-Qi, Li Wen-Jie, Xing Xiu-Na, Li Hai-Yang, He Pi-Mo, Bao Shi-Ning and Li Hong-Nian

CONDENSED MATTER: ELECTRONIC STRUCTURE, ELECTRICAL, MAGNETIC, AND OPTI-**CAL PROPERTIES**

127101 Defect-induced ferromagnetism in rutile TiO₂: A first-principles study Zhang Yong, Qi Yue-Ying, Hu Ya-Hua and Liang Pei

127102 Ab initio investigation of the structural and unusual electronic properties of α -CuSe (klockmannite)

- Ali Reza Shojaei, Zahra Nourbakhsh, Aminollah Vaez and Mohammad Dehghani
- In situ electronic structural study of VO₂ thin film across the metal-insulator transition 127103 Emin Muhemmed, Abduleziz Ablat, Wu Rui, Wang Jia-Ou, Qian Hai-Jie and Kurash Ibrahim
- Anisotropic localization behavior of graphene in the presence of diagonal and off-diagonal disorders 127201 Wang Li-Min, Shi Shao-Cong and Zhang Wei-Yi
- 127302 Transport and magnetoresistance effect in an oxygen-deficient SrTiO₃/La_{0.67}Sr_{0.33}MnO₃ heterojunction Wang Jing, Chen Chang-Le, Yang Shi-Hai, Luo Bing-Cheng, Duan Meng-Meng and Jin Ke-Xin
- ORS 127303 Influence of annealing temperature on passivation performance of thermal atomic layer deposition Al₂O₃ films

Zhang Xiang, Liu Bang-Wu, Zhao Yan, Li Chao-Bo and Xia Yang

Politil Sales Increased performance of an organic light-emitting diode by employing a zinc phthalocyanine based 127304 composite hole transport layer

Guo Run-Da, Yue Shou-Zhen, Wang Peng, Chen Yu, Zhao Yi and Liu Shi-Yong

- 127305 Dependence of electron dynamics on magnetic fields in semiconductor superlattices Yang Gui, Wang Lei and Tian Jun-Long
- Post-annealing effect on the structural and mechanical properties of multiphase zirconia films deposited 127306 by a plasma focus device

I. A. Khan, R. S. Rawat, R. Ahmad and M. A. K. Shahid

A monolithic distributed phase shifter based on right-handed nonlinear transmission lines at 30 GHz 127307 Huang Jie, Zhao Qian, Yang Hao, Dong Jun-Rong and Zhang Hai-Ying

- 127401 Switching effects in superconductor/ferromagnet/superconductor graphene junctions Li Xiao-Wei, Liu Dan and Bao Yan-Hui 127501 Phase transition in a two-dimensional Ising ferromagnet based on the generalized zero-temperature **Glauber dynamics** Meng Qing-Kuan, Feng Dong-Tai, Gao Xu-Tuan and Mei Yu-Xue 127801 Phase shift of polarized light through sculptured thin films: Experimental measurements and theoretical study Hou Yong-Qiang, Qi Hong-Ji, Li Xu, He Kai, Yi Kui and Shao Jian-Da 127802 Interplay between out-of-plane magnetic plasmon and lattice resonance for modified resonance lineshape and near-field enhancement in double nanoparticles array Ding Pei, Wang Jun-Qiao, He Jin-Na, Fan Chun-Zhen, Cai Gen-Wang and Liang Er-Jun INTERDISCIPLINARY PHYSICS AND RELATED AREAS OF SCIENCE AND TECHNOLOGY
- Fabrication and performance optimization of Mn-Zn ferrite/EP composites as microwave absorbing 128101 materials

Wang Wen-Jie, Zang Chong-Guang and Jiao Qing-Jie

Size-dependent thermal stresses in the core-shell nanoparticles 128102

Astefanoaei I, Dumitru I and Stancu Al

128201 Theoretical prediction of the optimal conditions for observing the stereodynamical vector properties of the C(³P) + OH (X² Π) \rightarrow CO(X¹ Σ ⁺) + H(²S) reaction

Wang Yuan-Peng, Zhao Mei-Yu, Yao Shun-Huai, Song Peng and Ma Feng-Cai

128401 **Cubature Kalman filters: Derivation and extension**

Zhang Xin-Chun and Guo Cheng-Jun

- 128402 Effects of NPB anode buffer layer on charge collection in ZnO/MEH-PPV hybrid solar cells Gong Wei, Xu Zheng, Zhao Su-Ling, Liu Xiao-Dong, Fan Xing, Yang Qian-Qian and Kong Chao
- PRS 128403 Alternating-current losses in two-layer superconducting cables consisting of second-generation superconductors coated by U-shaped ferromagnetic materials

Ahmet Cicek, Fedai Inanir and Fedor Gömöry

- 128501 Multichannel fetal magnetocardiography using SQUID bootstrap circuit Zhang Shu-Lin, Zhang Guo-Feng, Wang Yong-Liang, Liu Ming, Li Hua, Qiu Yang, Zeng Jia, Kong Xiang-Yan and Xie Xiao-Ming
- Improvement in electroluminescence performance of n-ZnO/Ga2O3/p-GaN heterojunction light-128502 emitting diodes

Zhang Li-Chun, Zhao Feng-Zhou, Wang Fei-Fei and Li Qing-Shan

- 0.15-µm T-gate In_{0.52}Al_{0.48}As/In_{0.53}Ga_{0.47}As InP-based HEMT with fmax of 390 GHz 128503 Zhong Ying-Hui, Zhang Yu-Ming, Zhang Yi-Men, Wang Xian-Tai, Lü Hong-Liang, Liu Xin-Yu and Jin Zhi
- Open critical area model and extraction algorithm based on the net flow-axis 128504 Wang Le, Wang Jun-Ping, Gao Yan-Hong, Xu Dan, Li Bo-Bo and Liu Shi-Gang

- **128505** Organic photovoltaic cells with copper (II) tetra-methyl substituted phthalocyanine Xu Zong-Xiang and Roy V. A. L.
- 128506 Flexible white top-emitting organic light-emitting diode with a MoO_x roughness improvement layer Chen Shu-Fen, Guo Xu, Wu Qiang, Zhao Xiao-Fei, Shao Ming and Huang Wei
- **128701** Symmetrical adhesion of two cylindrical colloids to a tubular membrane Niu Yu-Quan, Wei Wei, Zheng Bin, Zhang Cai-Xia and Meng Qing-Tian
- **128702** Species diversity in rock–paper–scissors game coupling with Levy flight Wang Dong, Zhuang Qian, Fan Ying and Di Zeng-Ru
- 128901 Stochastic bounded consensus tracking of leader-follower multi-agent systems with measurement noises based on sampled data with general sampling delay Wu Zhi-Hai, Peng Li, Xie Lin-Bo and Wen Ji-Wei

GEOPHYSICS, ASTRONOMY, AND ASTROPHYSICS

- **129201** Ground-based remote sensing of atmospheric total column CO₂ and CH₄ by direct sunlight in Hefei Cheng Si-Yang, Xu Liang, Gao Min-Guang, Li Sheng, Jin Ling, Tong Jing-Jing, Wei Xiu-Li, Liu Jian-Guo and Liu Wen-Qing
- 129202 Analysis of stable components in the extended-range forecast for the coming 10–30 days in winter 2010 and 2011

Wang Kuo, Feng Guo-Lin, Zeng Yu-Xing and Wang Xu-Jia

- **129401** Modulational instability of optically induced nematicon propagation L. Kavitha, M. Venkatesh, S. Dhamayanthi and D. Gopi
- **129402** Transcription's bubble under the influence of long-range interactions and helicoidal coupling Mirabeau Saha and Timoléon C. Kofané
- 129701 Electron capture rates for iron group nuclei at the surface of magnetar

Luo Xia, Du Jun and Li Ping-Ping